ECE 6345

Spring 2015

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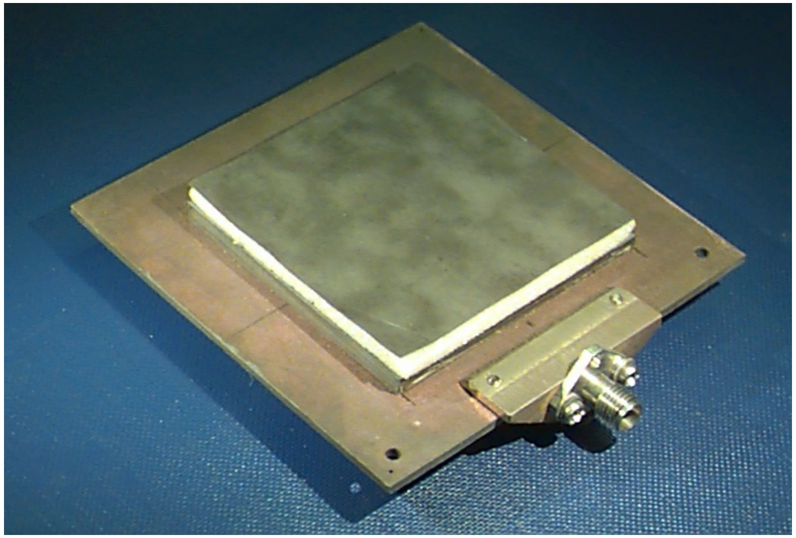
ECE Dept.



Notes 6

Overview

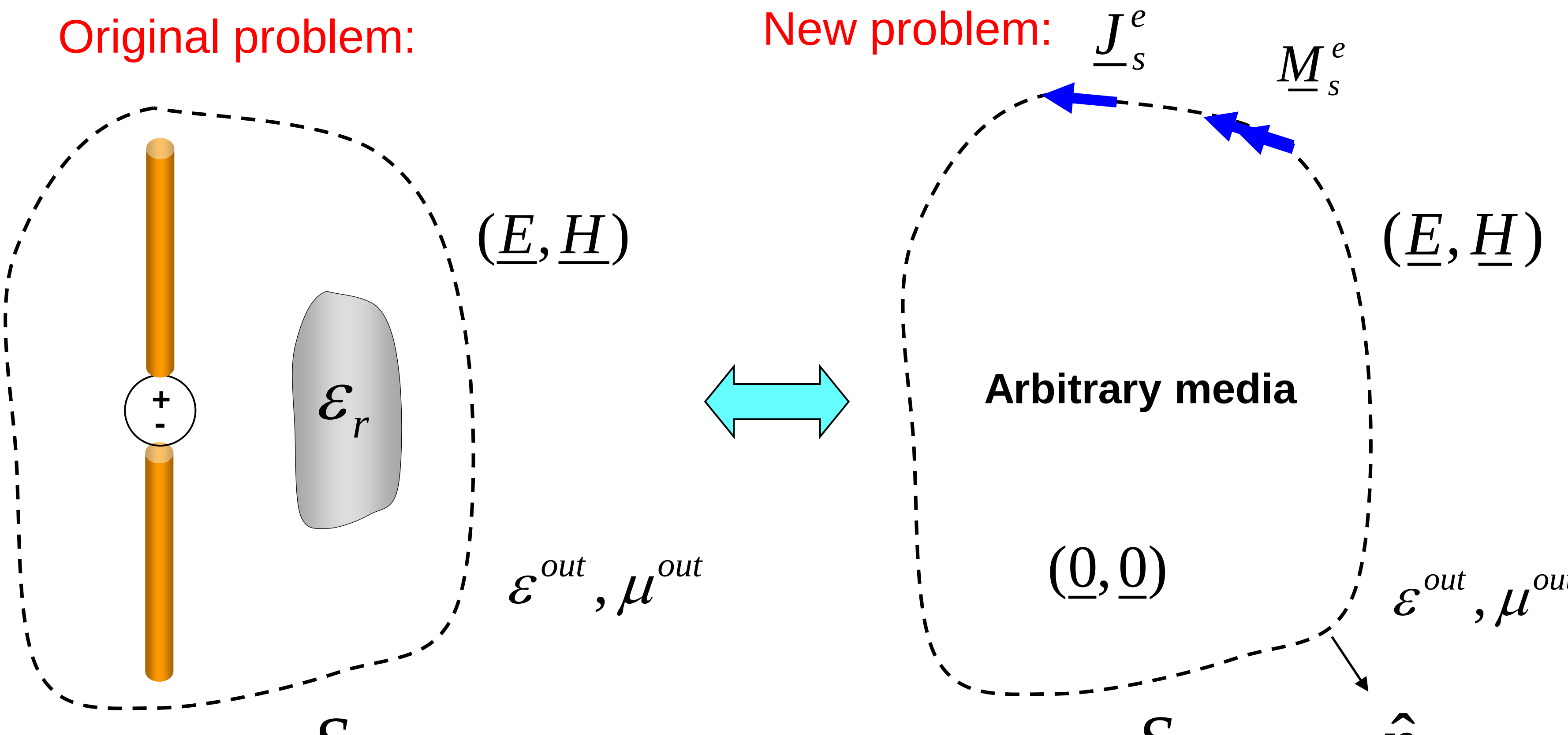
In this set of notes we look at two different models for calculating the radiation pattern of a microstrip antenna:

- Electric current model
- Magnetic current model

We also look at two different substrate assumptions:

- Infinite substrate
- Truncated substrate (truncated at the edge of the patch).

Review of Equivalence Principle

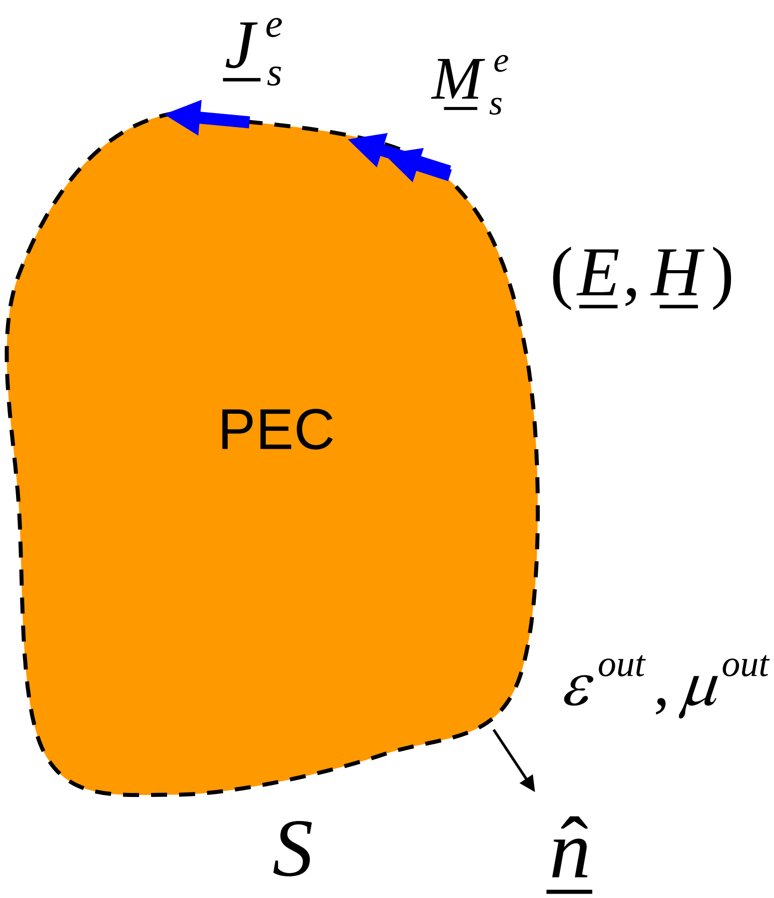


$$\underline{J}_s^e = \underline{\hat{n}} \times \underline{H}$$

$$\underline{M}_s^e = -\underline{\hat{n}} \times \underline{E}$$

Review of Equivalence Principle

A common choice (PEC inside):

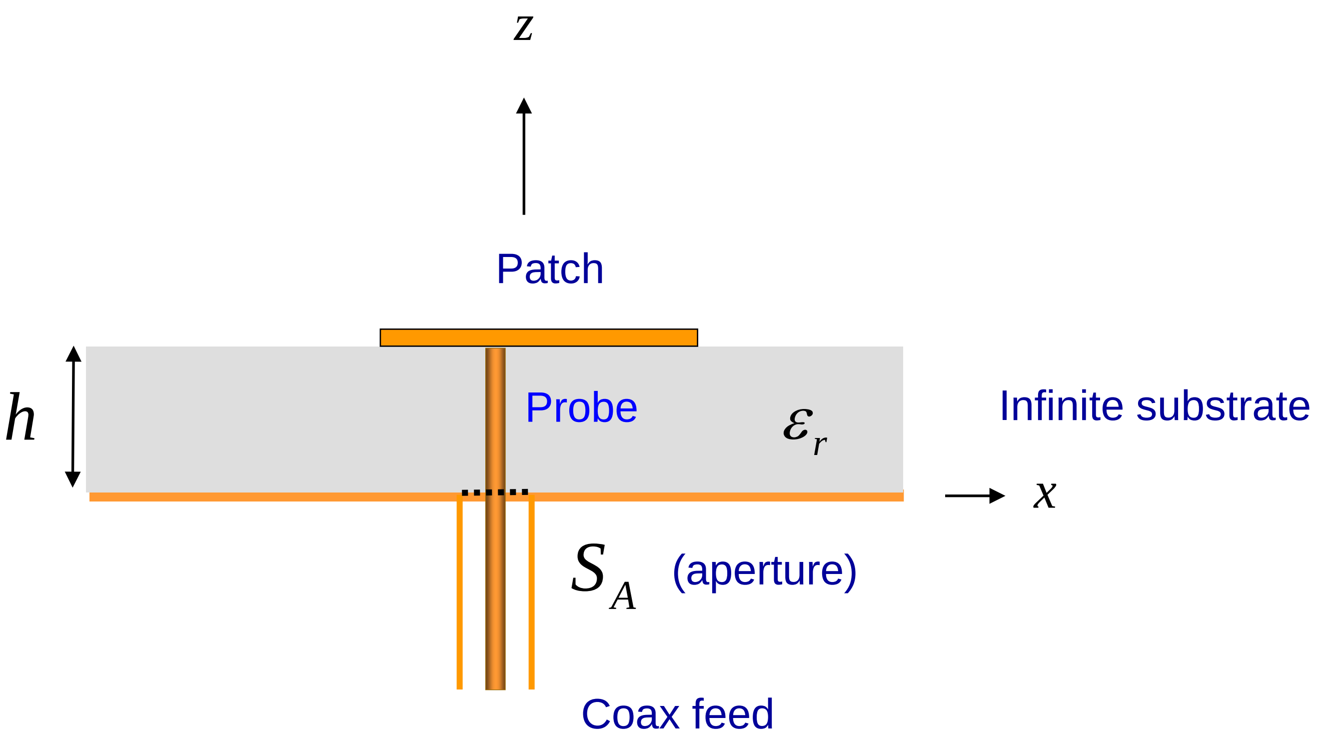


The electric surface current sitting on the PEC object does not radiate, and can be ignored.

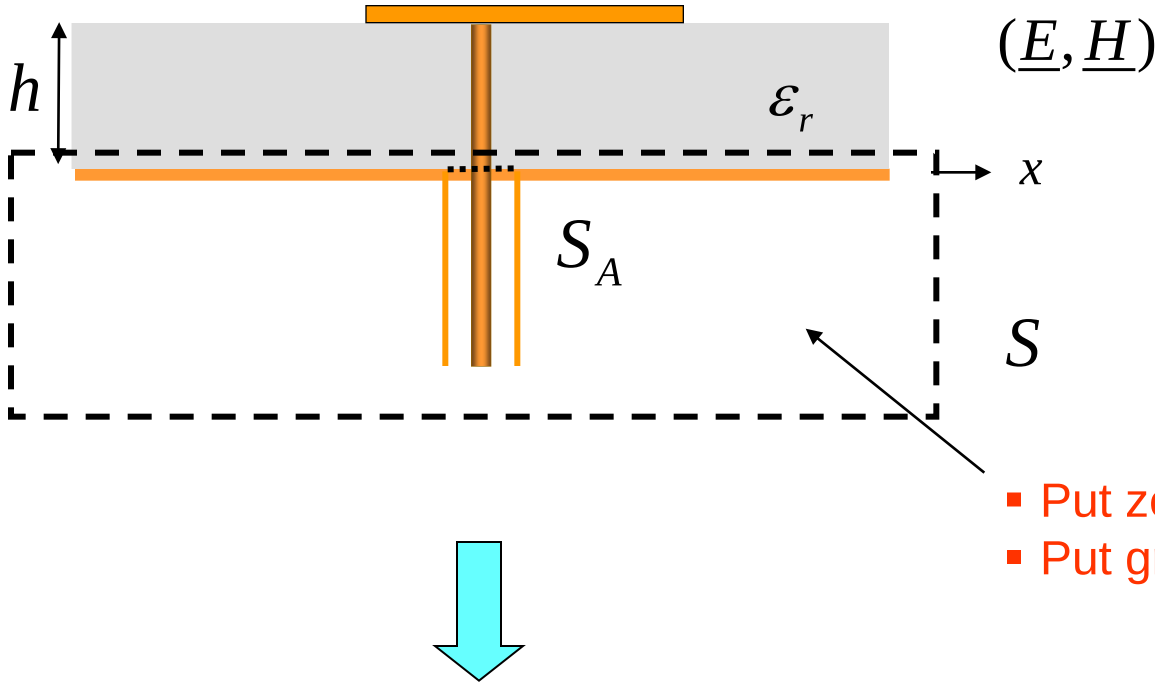
$$\underline{J}_s^e = \underline{\hat{n}} \times \underline{H}$$

$$\underline{M}_s^e = -\underline{\hat{n}} \times \underline{E}$$

Model of Patch and Feed



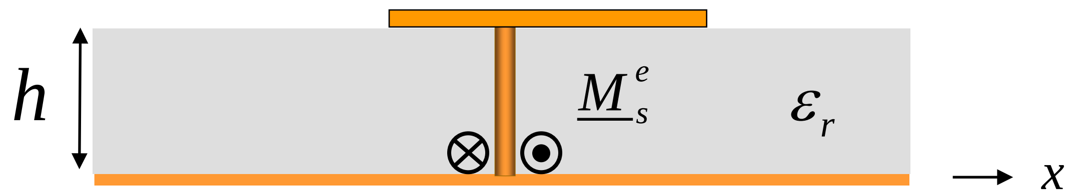
Model of Patch and Feed



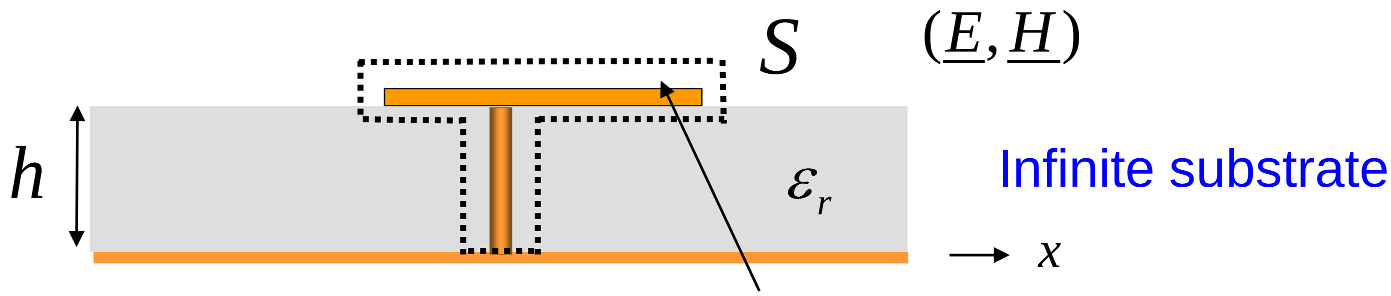
- Put zero fields
- Put ground plane

Magnetic frill model:

Aperture: $\underline{M}_s^e = -\underline{\hat{z}} \times \underline{E}$



Electric Current Model: Infinite Substrate



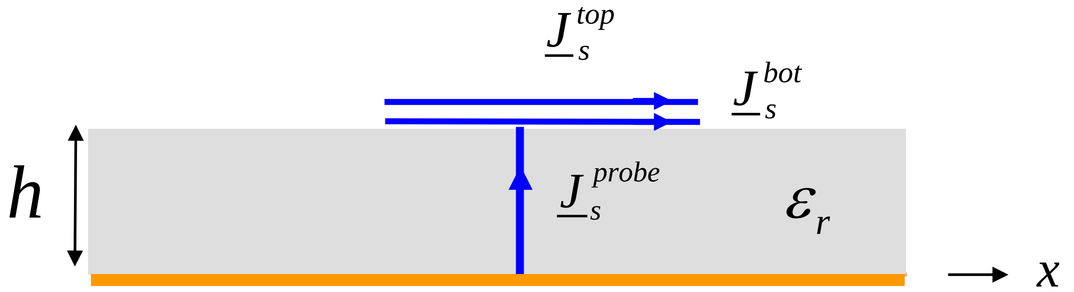
The surface S "hugs" the PEC metal.

- Put zero fields
- Remove patch and probe

Note: The frill is ignored.

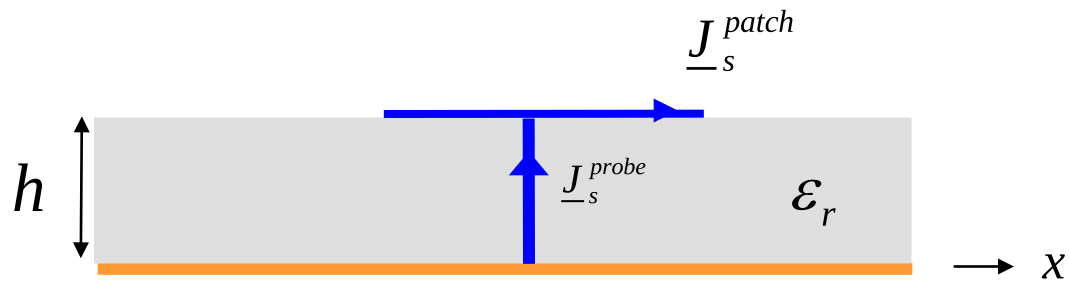
$$\underline{M}_s^e = -\underline{\hat{n}} \times \underline{E} = -\underline{\hat{n}} \times \underline{E}_t = \underline{0}$$

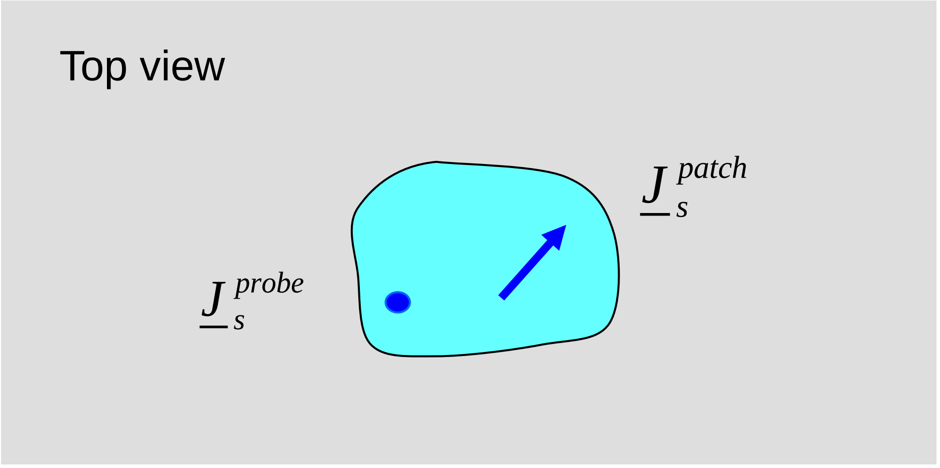
$$\underline{J}_s^e = \underline{\hat{n}} \times \underline{H} = \underline{J}_s$$



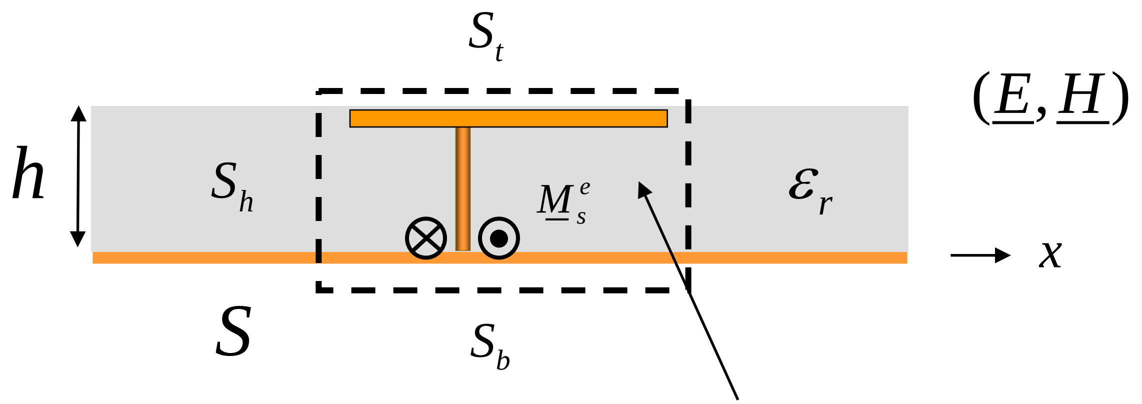
Electric Current Model: Infinite Substrate (cont.)

Let $\underline{J}_s^{patch} = \underline{J}_s^{top} + \underline{J}_s^{bot}$





Magnetic Current Model: Infinite Substrate



- Put zero fields
- Remove patch, probe, and frill current
- Put substrate and ground plane

$$\underline{M}_s^e = -\underline{\hat{n}} \times \underline{E} = \underline{0}, \qquad \underline{r} \in S_t, S_b$$

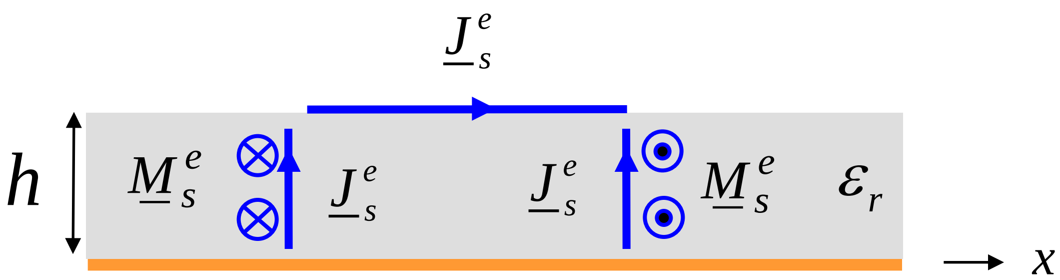
$$\underline{J}_s^e = +\underline{\hat{n}} \times \underline{H} = \underline{0}, \qquad \underline{r} \in S_b$$

$$\underline{J}_s^e \approx \underline{0}, \qquad \underline{r} \in S_t$$ (weak fields)

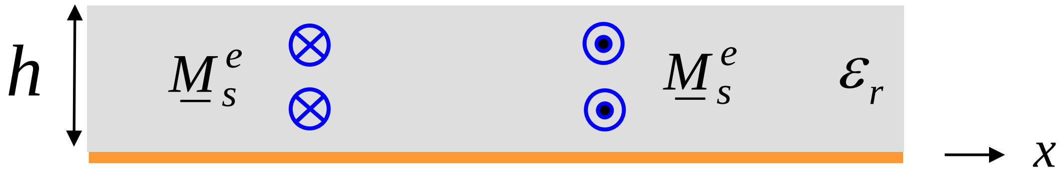
$$\underline{J}_s^e \approx \underline{0}, \qquad \underline{r} \in S_h$$ (approximate PMC)

Magnetic Current Model: Infinite Substrate (cont.)

Exact model:



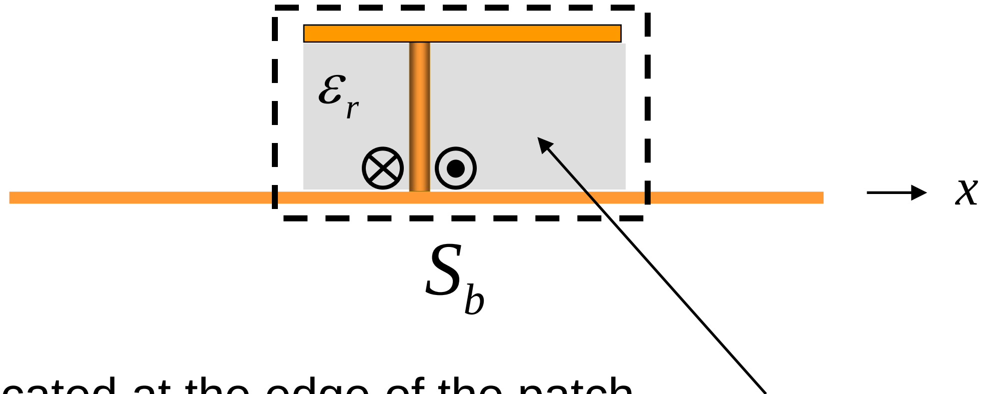
Approximate model:



$$\underline{M}_s^e = -\underline{\hat{n}} \times \underline{E}$$

Note: The magnetic currents radiate inside an infinite substrate above a ground plane.

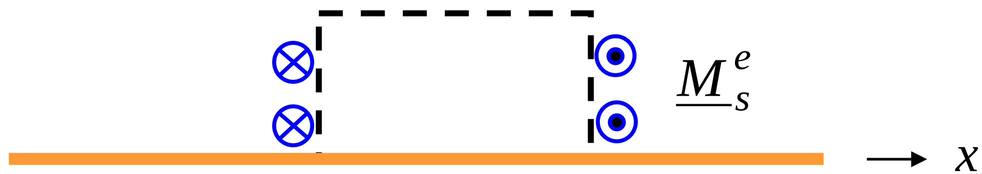
Magnetic Current Model: Truncated Substrate



The substrate is truncated at the edge of the patch.

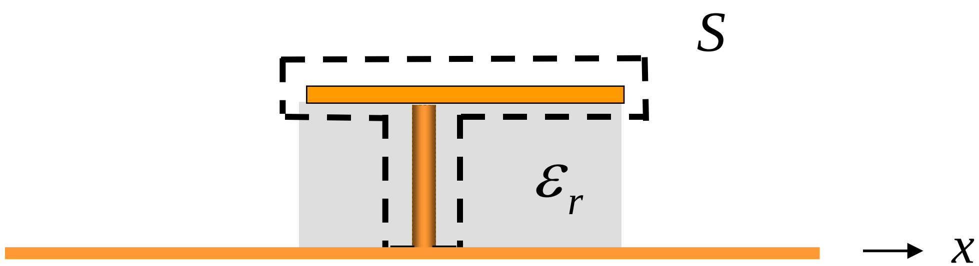
- Put zero fields
- Remove the substrate

Approximate model:



Note: The magnetic currents radiate in free space above a ground plane.

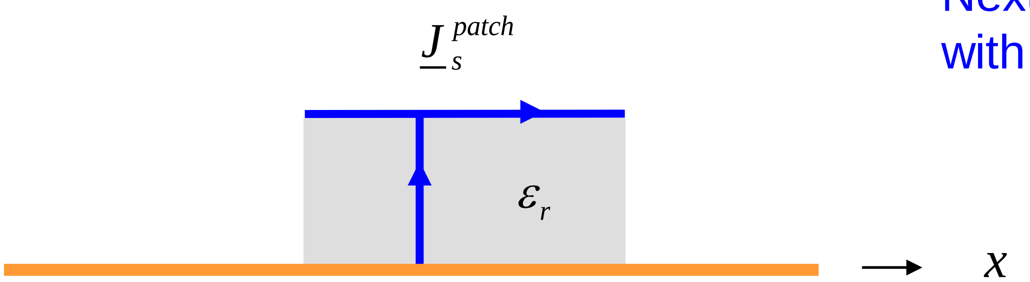
Electric Current Model: Truncated Substrate



The patch and probe are replaced by surface currents, as before.

The substrate is truncated at the edge of the patch.

$$\underline{J}_s^{patch} = \underline{J}_s^{top} + \underline{J}_s^{bot}$$



Next, we replace the dielectric with *polarization currents*.

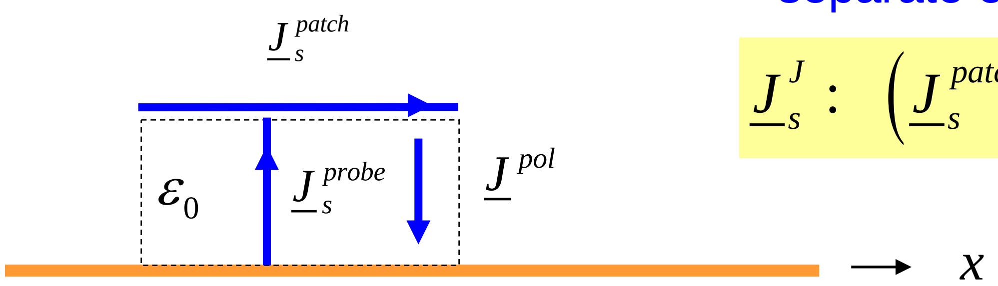
Electric Current Model: Truncated Substrate (cont.)

$$\nabla \times \underline{H} = j\omega\varepsilon\underline{E}$$
$$= j\omega(\varepsilon - \varepsilon_0)\underline{E} + j\omega\varepsilon_0\underline{E}$$
$$= j\omega\varepsilon_0(\varepsilon_r - 1)\underline{E} + j\omega\varepsilon_0\underline{E}$$

$$\Rightarrow \quad \underline{J}^{pol} = j\omega\varepsilon_0(\varepsilon_r - 1)\underline{E}$$

In this model we have three separate electric currents.

$$\underline{J}_s^J : \left(\underline{J}_s^{patch},\ \underline{J}_s^{probe},\ \underline{J}^{pol}\right)$$



Comments on Models

Infinite Substrate

- The electric current model is exact (if we neglect the frill), but it requires knowledge of the exact patch and probe currents.
- The magnetic current model is approximate, but fairly simple.
- For a rectangular patch, both models are fairly simple if only the (1,0) mode is assumed.
- For a circular patch, the magnetic current model is much simpler (it does not involve Bessel functions).

Comments on Models (cont.)

Truncated Substrate

- The electric current model is exact (if we neglect the frill), but it requires knowledge of the exact patch and probe currents, as well as the field inside the patch cavity (to get the polarization currents). It is a complicated model.
- The magnetic current model is approximate, but very simple. This is the recommended model.
- For the magnetic current model the same formulation applies as for the infinite substrate – the substrate is simply taken to be air.

Theorem

The electric and magnetic models yield identical results at the resonance frequency of the cavity mode.

Assumptions:

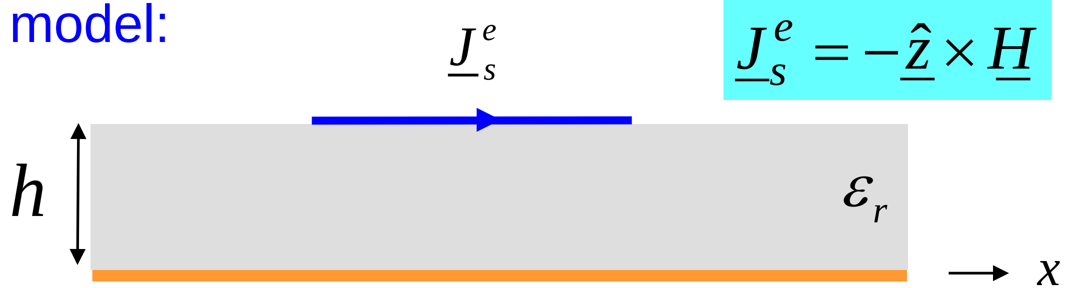
1) The electric and magnetic current models are based on the fields of a *single cavity mode corresponding to an ideal lossless cavity with PMC walls*.
2) The probe current is neglected in the electric current model.

Note: This theorem is true for either infinite or truncated substrates.

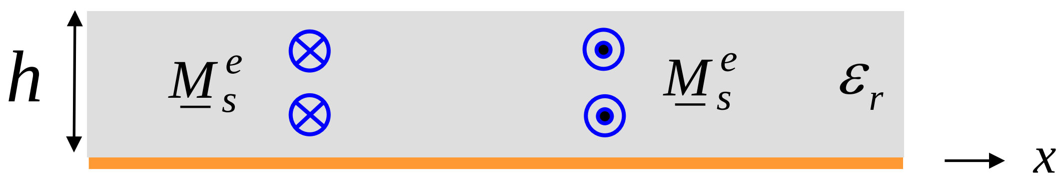
Theorem (cont.)

Electric-current model:

$$\underline{J}_s^e = -\underline{\hat{z}} \times \underline{H}$$



Magnetic-current model:



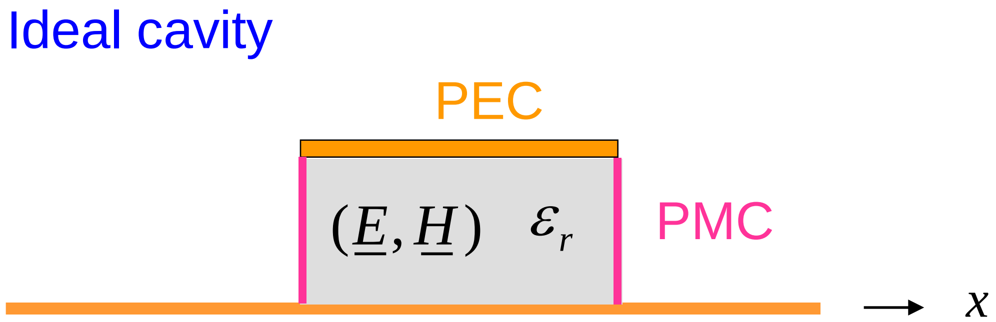
$$\underline{M}_s^e = -\underline{\hat{n}} \times \underline{E}$$

($\underline{E}$, $\underline{H}$) = fields of resonant cavity mode with PMC side walls

Theorem (cont.)

Proof:

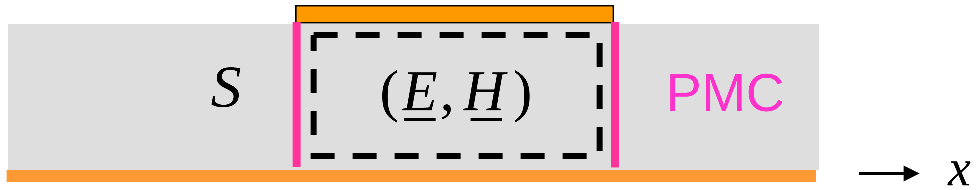
We start with an ideal cavity having PMC walls on the sides. This cavity will support a valid non-zero set of fields at the resonance frequency f_0 of the mode.



At $f = f_0 : \quad (\underline{E}, \underline{H}) \neq (\underline{0}, \underline{0})$

Proof

Proof for infinite substrate

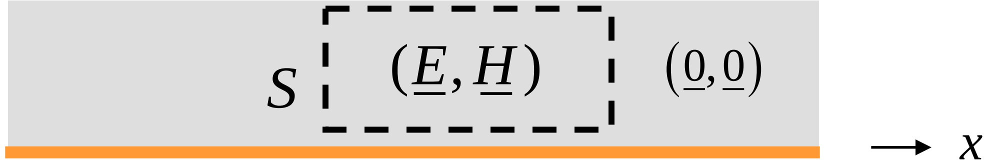


Equivalence principle:

Put $(\underline{0}, \underline{0})$ outside S

Keep $(\underline{E}, \underline{H})$ inside S

The PEC and PMC walls have been removed in the zero field (outside) region. We keep the substrate and ground plane in the outside region.

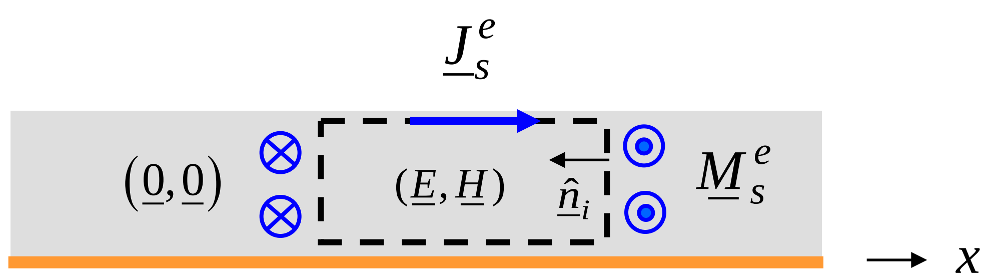


Proof (cont.)

$$\underline{J}_s^e = \underline{\hat{n}}_i \times \underline{H}$$

$$\underline{M}_s^e = -\underline{\hat{n}}_i \times \underline{E}$$

Note the inward pointing normal $\underline{\hat{n}}_i$



Note: The electric current on the ground is neglected (it does not radiate).

Proof (cont.)

Exterior Fields:

$$\underline{E}^{+}\left[\underline{J}_s^e\right]+\underline{E}^{+}\left[\underline{M}_s^e\right]=\underline{0}$$

$$\underline{J}_s^e=\underline{\hat{n}}_i\times\underline{H}=-\underline{\hat{z}}\times\underline{H}=\underline{J}_s^{patch}=\underline{J}_s^J$$

(The equivalent electric current is the same as the electric current in the electric current model.)

$$\begin{aligned}\underline{M}_s^e&=-\underline{\hat{n}}_i\times\underline{E}\\&=+\underline{\hat{n}}\times\underline{E}\\&=-\left(-\underline{\hat{n}}\times\underline{E}\right)\\&=-\underline{M}_s^M\end{aligned}$$

(The equivalent current is the negative of the magnetic current in the magnetic current model.)

Proof (cont.)

Hence

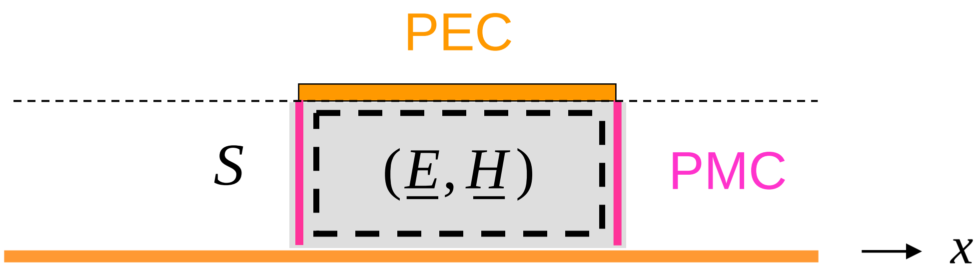
$$\underline{E}^{+}\left[\underline{J}_{s}^{J}\right]+\underline{E}^{+}\left[-\underline{M}_{s}^{M}\right]=\underline{0}$$

or

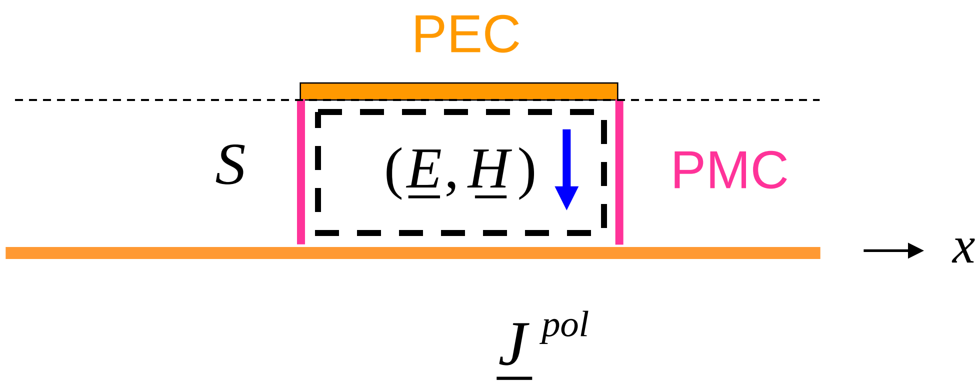
$$\underline{E}^{+}\left[\underline{J}_{s}^{J}\right]=\underline{E}^{+}\left[\underline{M}_{s}^{M}\right]$$

Theorem for Truncated Substrate

Proof for truncated model



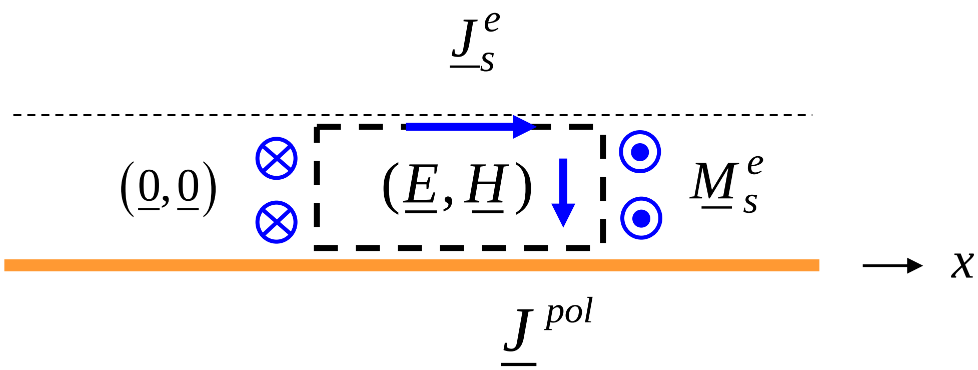
Replace the dielectric with polarization current:



Proof (cont.)

$$\underline{J}_s^{\,e} = \underline{J}_s^{\,patch}$$

$$\underline{M}_s^{\,e} = -\underline{M}_s^{\,M}$$



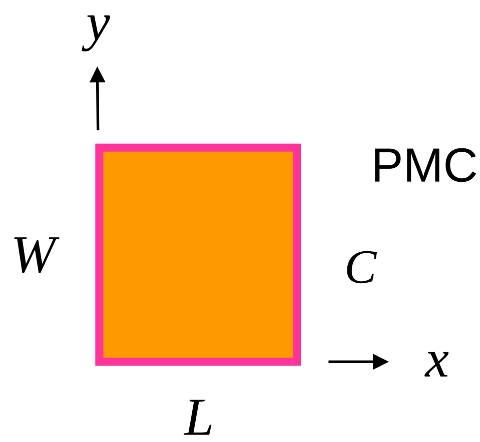
$$\underline{E}^{+}\left[\underline{J}_s^{\,patch}\right] + \underline{E}^{+}\left[\underline{J}^{\,pol}\right] + \underline{E}^{+}\left[-\underline{M}_s^{\,M}\right] = 0$$

or $$\underline{E}^{+}\left[\underline{J}_s^{\,patch}\right] + \underline{E}^{+}\left[\underline{J}^{\,pol}\right] = \underline{E}^{+}\left[\underline{M}_s^{\,M}\right]$$

Hence $$\underline{E}^{+}\left[\underline{J}_s^{\,J}\right] = \underline{E}^{+}\left[\underline{M}_s^{\,M}\right]$$

Rectangular Patch

Ideal cavity model:



$$\left.\frac{\partial E_z}{\partial n} = 0\right|_C$$

$$\nabla^2 E_z + k^2 E_z = 0$$

Let $E_z(x,y) = X(x)\,Y(y)$

$$X''Y + XY'' + k^2 XY = 0$$

Divide by $X(x)Y(y)$: $\dfrac{X''}{X} + \dfrac{Y''}{Y} + k^2 = 0$

so $\dfrac{X''}{X} = -\left(k^2 + \dfrac{Y''}{Y}\right)$

Rectangular Patch (cont.)

Hence

$$\frac{X''(x)}{X(x)} = \text{constant} \equiv -k_x^2$$

General solution: $X(x) = A\sin k_x x + B\cos k_x x$

Boundary condition: $X'(0) = k_x A\cos(k_x 0) - k_x B\sin(k_x 0) = k_x A = 0$

$\Rightarrow$ $A = 0$

Choose $B = 1$

$$X(x) = \cos(k_x x)$$

Boundary condition: $X'(L) = -k_x \sin\left(k_x L\right) = 0$

$$\Rightarrow \quad k_x = \frac{m\pi}{L}$$

Rectangular Patch (cont.)

so $$X(x) = \cos\left(\frac{m\pi x}{L}\right)$$

Returning to the Helmholtz equation, $-k_x^2 + \frac{Y''}{Y} + k^2 = 0$

so $$\frac{Y''}{Y} = \text{constant} = -\left(k^2 - k_x^2\right) \equiv -k_y^2$$

Following the same procedure as for the $X(x)$ function, we have:

$$Y(y) = \cos\left(\frac{n\pi y}{W}\right)$$

Hence $$E_z^{(m,n)}(x,y) = \cos\left(\frac{m\pi x}{L}\right)\cos\left(\frac{n\pi y}{W}\right)$$

Rectangular Patch (cont.)

Using $-k_x^2 - k_y^2 + k^2 = 0$

we have $$k_{mn} = \sqrt{\left(\frac{m\pi}{L}\right)^2 + \left(\frac{n\pi}{W}\right)^2}$$

where $k_{mn} = \omega_{mn}\sqrt{\mu\varepsilon}$

Hence $$\omega_{mn} = \frac{1}{\sqrt{\mu\varepsilon}}\sqrt{\left(\frac{m\pi}{L}\right)^2 + \left(\frac{n\pi}{W}\right)^2}$$

$$\omega_{mn} = \frac{c}{\sqrt{\varepsilon_r}}\sqrt{\left(\frac{m\pi}{L}\right)^2 + \left(\frac{n\pi}{W}\right)^2}$$

Rectangular Patch (cont.)

Current:

$$\underline{J}_s^{\,patch} = \underline{\hat{n}} \times \underline{H} = -\underline{\hat{z}} \times \underline{H}$$

$$\underline{H} = \frac{-1}{j\omega\mu} \nabla \times \underline{E}$$

$$= \frac{-1}{j\omega\mu} \nabla \times \left(\underline{\hat{z}}\, E_z \right)$$

$$= \frac{-1}{j\omega\mu} \left[\left(\nabla \times \underline{\hat{z}} \right) E_z - \underline{\hat{z}} \times \nabla E_z \right]$$

so

$$\underline{H} = \frac{1}{j\omega\mu} \left(\underline{\hat{z}} \times \nabla E_z \right)$$

Rectangular Patch (cont.)

Hence

$$\underline{J}_s^{patch} = -\frac{1}{j\omega\mu}\underline{\hat{z}} \times \left(\underline{\hat{z}} \times \nabla E_z\right) \quad \Rightarrow \quad \underline{J}_s^{patch} = \frac{1}{j\omega\mu}\nabla E_z$$

$$\underline{J}_s^{patch} = \frac{1}{j\omega\mu}\left[\underline{\hat{x}}\left(-\frac{m\pi}{L}\right)\sin\left(\frac{m\pi x}{L}\right)\cos\left(\frac{n\pi y}{W}\right) + \underline{\hat{y}}\left(-\frac{n\pi}{W}\right)\cos\left(\frac{m\pi x}{L}\right)\sin\left(\frac{n\pi y}{W}\right)\right]$$

Dominant (1,0) Mode:

$$E_z(x, y) = \cos\left(\frac{\pi x}{L}\right)$$

$$\underline{J}_s(x, y) = -\underline{\hat{x}}\left(\frac{1}{j\omega\mu}\right)\left(\frac{\pi}{L}\right)\sin\left(\frac{\pi x}{L}\right)$$

Rectangular Patch (cont.)

Static (0,0) mode:

$$E_z(x,y) = 1$$

$$\omega_{00} = 0$$

$$\underline{J}_s(x,y) = \underline{0}$$

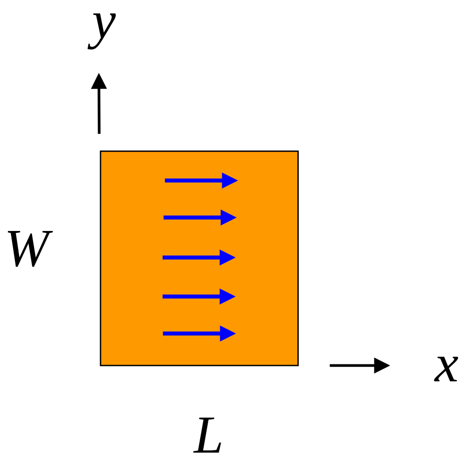
This is a "static capacitor" mode.

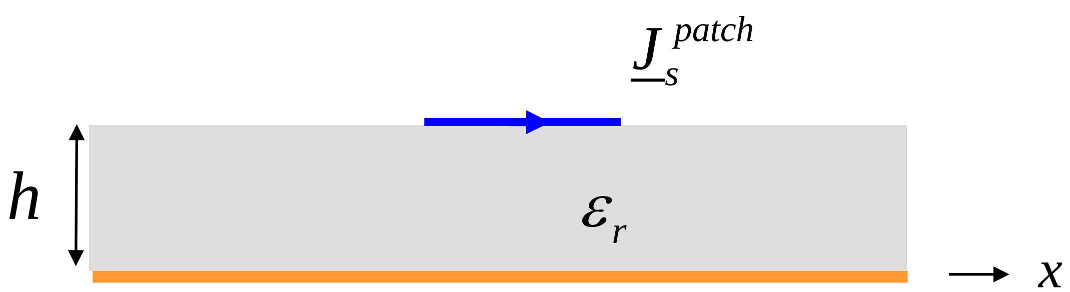
A patch operating in this mode does not radiate at zero frequency, but it can be made resonant at a higher frequency if the patch is loaded by an inductive probe (a good way to make a miniaturized patch).

Radiation Model for (1,0) Mode

Electric-current model:

$$\underline{J}_s^{patch} = -\underline{\hat{x}}\left(\frac{\pi}{j\omega\mu L}\right)\sin\left(\frac{\pi x}{L}\right)$$





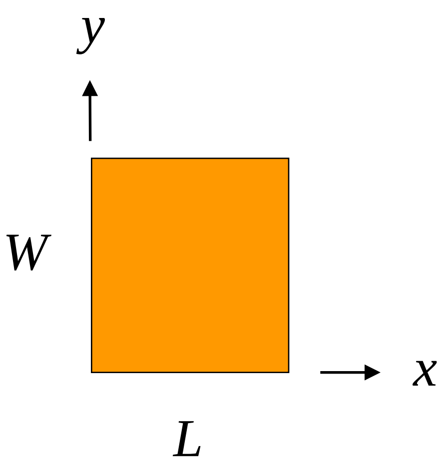
Radiation Model for (1,0) Mode (cont.)

Magnetic-current model:

$$\underline{M}_s^M = -\underline{\hat{n}} \times \underline{E}$$

$$= -\underline{\hat{n}} \times \left[\underline{\hat{z}} \cos\left(\frac{\pi x}{L}\right) \right]$$

$$\underline{\hat{n}} = \begin{cases} \underline{\hat{x}} & x = L \\ -\underline{\hat{x}} & x = 0 \\ \underline{\hat{y}} & y = W \\ -\underline{\hat{y}} & y = 0 \end{cases}$$

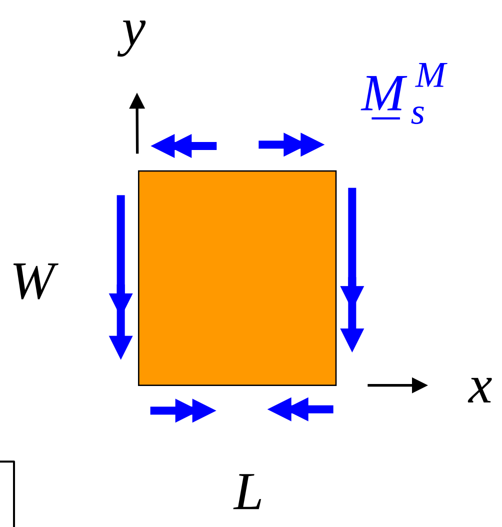


Radiation Model for (1,0) Mode (cont.)

Hence

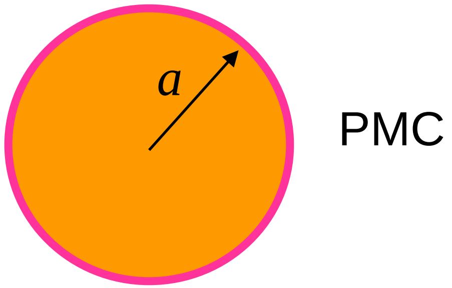
$$\underline{M}_s^M = \begin{cases} \underline{\hat{y}}\cos\pi = -\underline{\hat{y}} & x = L \\ -\underline{\hat{y}}\cos 0 = -\underline{\hat{y}} & x = 0 \\ -\underline{\hat{x}}\cos\left(\dfrac{\pi x}{L}\right) & y = W \\ \underline{\hat{x}}\cos\left(\dfrac{\pi x}{L}\right) & y = 0 \end{cases}$$

radiating edges



The non-radiating edges do not contribute to the far-field pattern in the principal planes.

Circular Patch



$$\nabla^2 E_z + k^2 E_z = 0$$

$$E_z = \begin{pmatrix} J_n(k_\rho \rho) \\ \cancel{Y_n(k_\rho \rho)} \end{pmatrix} \begin{pmatrix} \cos(n\phi) \\ \sin(n\phi) \end{pmatrix} \cos\left(\frac{m\pi z}{h}\right)$$

set $m = 0$ ⟹

$$k_\rho = \left(k^2 - k_z^2\right)^{1/2} = \left(k^2 - \left(\frac{m\pi}{h}\right)^2\right)^{1/2} = k$$

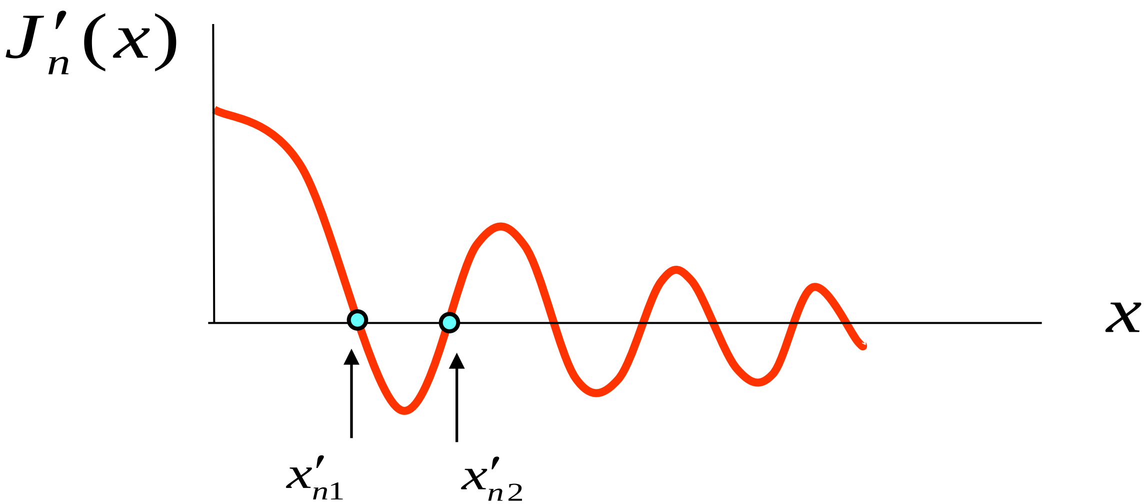
Circular Patch (cont.)

Note: $\cos\phi$ and $\sin\phi$ modes are degenerate (same resonance frequency).

Choose $\cos\phi$: $E_z = \cos(n\phi) J_n(k\rho)$

$$\left.\frac{\partial E_z}{\partial \rho} = 0\right|_{\rho=a}$$

$$J_n'(ka) = 0$$



Circular Patch (cont.)

Hence $$ka = x'_{np}$$

so $$\omega_{np} = \frac{c}{\sqrt{\varepsilon_r}} x'_{np}$$

Dominant mode (lowest frequency) is TM_{11}:

$$(n, p) = (1,1)$$

$$x'_{11} = 1.841$$

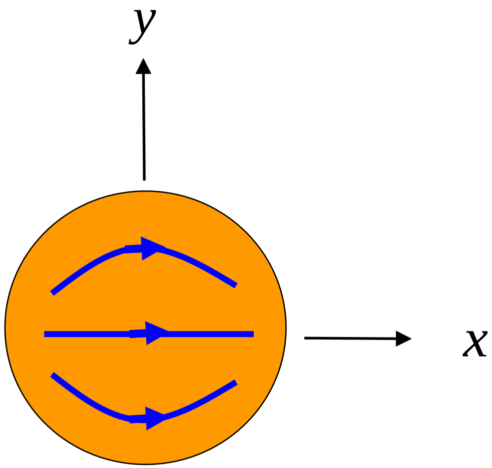
$$E_z^{(1,1)}(\rho, \phi) = \cos\phi \, J_1(k\rho)$$

Circular Patch (cont.)

Electric current model:

$$\underline{J}_s^J = \frac{1}{j\omega\mu}\nabla E_z = \frac{1}{j\omega\mu}\left(\underline{\hat{\rho}}\frac{\partial E_z}{\partial \rho} + \underline{\hat{\phi}}\frac{1}{\rho}\frac{\partial E_z}{\partial \phi}\right)$$

$$= \frac{1}{j\omega\mu}\left[\underline{\hat{\rho}}\, k \cos n\phi \; J_n'(k\rho) + \underline{\hat{\phi}}\frac{1}{\rho}(-n)\sin n\phi \; J_n(k\rho)\right]$$



TM$_{11}$ mode:

$$n = 1, \; p = 1$$

$$\underline{J}_s^J = -\frac{1}{j\omega\mu}\left[\underline{\hat{\rho}}\, k \cos\phi \; J_1'(k\rho) - \underline{\hat{\phi}}\frac{1}{\rho}\sin\phi \; J_1(k\rho)\right]$$

Very complicated!

Circular Patch (cont.)

Magnetic current model:

$$\underline{M}_s^M = -\underline{\hat{n}} \times \underline{E}$$
$$= -\underline{\hat{\rho}} \times \left(\underline{\hat{z}}\, E_z \right)$$
$$= \underline{\hat{\phi}}\, E_z$$

so

$$\underline{M}_s^M = \underline{\hat{\phi}} \cos n\phi \, J_n(ka)$$

TM_{11}: $n = 1,\ p = 1$

$$\underline{M}_s^M = \underline{\hat{\phi}} \cos \phi \, J_1(ka)$$

Circular Patch (cont.)

Note: $V(\phi) = -h\,E_z(\phi)\Big|_{\rho=a}$

$$= -h\cos\phi \; J_1(ka)$$

At $\phi = 0$ $\quad V(0) \equiv V_0 = -h\,J_1(ka)$

Hence $\underline{M}_s^M = \underline{\hat{\phi}}\cos\phi\,J_1(ka) = \underline{\hat{\phi}}\cos\phi\left(-\dfrac{V_0}{h}\right)$

so

$$\underline{M}_s^M = -\underline{\hat{\phi}}\left(\frac{V_0}{h}\right)\cos\phi$$

Circular Patch (cont.)

Ring approximation: $\underline{K} = \underline{\hat{\phi}} K_\phi$

$$K_\phi = \int_0^h M_{s\phi}^M \, dz = h \, M_{s\phi}^M = h \cos\phi \left(-\frac{V_0}{h} \right) = -V_0 \cos\phi$$

$$K_\phi(\phi) = -V_0 \cos\phi$$